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## A wavelet-based dynamic mode decomposition for modeling mechanical systems from partial observations

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### ABSTRACT

Dynamic mode decomposition (DMD) has emerged as a popular data-driven modeling approach to identifying spatio-temporal coherent structures in dynamical systems, owing to its strong relation with the Koopman operator. For dynamical systems with external forcing, the identified model should not only be suitable for a specific forcing function but should generally approximate the input–output behavior of the underlying dynamics. A novel methodology for modeling those classes of dynamical systems is proposed in the present work, using wavelets in conjunction with the input–output dynamic mode decomposition (ioDMD). The wavelet-based dynamic mode decomposition (WDMD) builds on the ioDMD framework without the restrictive assumption of full state measurements. Our non-intrusive approach constructs numerical models directly from trajectories of the full model's inputs and outputs, without requiring the full-model operators. These trajectories are generated by running a simulation of the full model or observing the original dynamical systems' response to inputs in an experimental framework. Hence, the present methodology is applicable for dynamical systems whose internal state vector measurements are not available. Instead, data from only a few output locations are only accessible, as often the case in practice. The present methodology's applicability is explained by modeling the input–output response of an Euler–Bernoulli finite element beam model. The WDMD provides a linear state-space representation of the dynamical system using the response measurements and the corresponding input forcing functions. The developed state-space model can then be used to simulate the beam's response towards different types of forcing functions. The method is further validated on a real (experimental) data set using modal analysis on a simple free-free beam, demonstrating the efficacy of the proposed methodology as an appropriate candidate for modeling practical dynamical systems despite having no access to internal state measurements and treating the full model as a black-box.

### 1. Introduction

Over the last two decades, data-driven modeling has garnered interest in several research areas, particularly when the involved dynamics are complex and models based on first principles present challenges of varying degrees see, e.g., [1–9] and the references therein. Moreover, the advances in data processing and sensor capabilities made it much easier to map a system's response to a

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variety of inputs. In structural dynamics, structures vary in different levels of complexity, and physics-based models may not always be feasible [10–19]. To gain insight into the aforementioned class of dynamical systems and predict their behaviors in different operational or loading conditions, it is beneficial to create models using the measured input–output response data.

There are numerous techniques in literature to create mathematical models using the measured input–output response data, and system identification (SID) techniques are at the forefront of such methods [20,21]. In particular, the field of subspace-based system identification provides powerful tools for fitting a linear time-invariant (LTI) system to given input–output responses of the measured system [22–24]. The eigensystem realization algorithm (ERA) [25] is one of the most widely used SID techniques. In its original form, the ERA technique uses discrete time-impulse response function to approximate a linear time-invariant model of the original system. Starting with ERA, various versions have been proposed in the literature, replacing discrete time-impulse responses with various other output functions. For example: ERA-natural excitation technique (NeXT) [26,27] substitutes the impulse response with the correlation matrix of the output sensor data, and ERA-observer Kalman filter identification (OKID) [28,29] uses observer gain in place of impulse response functions. The stochastic subspace identification (SSI) is another popular technique for modal identification of dynamical systems, by projecting the future response onto the previous input/output response [30–32]. Furthermore, body of literature exists for modal identification of structural systems excited under earthquake ground motion using various linear and nonlinear SID techniques [33–36]. However, for mechanical systems with multiple sensors and actuators (MIMO), the SID and ERA techniques pose additional computational challenges. For example, ERA algorithm centers around a full singular-value decomposition (SVD) of a structured Hankel matrix, whose size scales linearly with the input and output dimension. Furthermore, in the case of systems with slowly decaying dynamics, large Hankel matrices are a possibility and handling them can be a challenge; see, e.g., [37,38], for recent works to resolve these potential computational bottlenecks.

Of late, dynamic mode decomposition (DMD) has become a popular tool in data-driven modeling, owing to its ability to decompose the high dimensional data into its coherent spatio-temporal structures [1,2,39–41]. DMD has its roots in the Koopman theory [42], whose work was later revived by seminal works of Mezić et al. [39–41,43–46]. Optimized DMD [47] and sparsity promoting DMD [48] transforms the approximation of the linear operator into an optimization problem with constraints in the eigenvalues, modes, or mode amplitudes. Multi-resolution DMD [49] and higher-order DMD [50] provide a recursive way to improve the frequency resolution and transient handling capability of the standard DMD. Kernel-based DMD [51] and Extended DMD (EDMD) [52] provide a means to extend the framework towards nonlinear systems by creating meaningful observables. Proctor et al. [53] developed a variant of DMD known as DMD with controls (DMDc) to incorporate the input signals into the DMD framework. Benner et al. [43] developed an extension of DMDc, known as input–output DMD (ioDMD), by providing means to incorporate outputs alongside inputs and states. The ioDMD and DMDc algorithm provide an elegant way to extend the standard DMD to include the effects of external forcing functions. Overall, the fundamental strength of DMD stems from its deep connection to the Koopman spectral theory [1,2,39,42], which provides the theoretical foundation and justification for applying DMD on linear [40,50,54–56] and nonlinear dynamics [51,57,58]. The flexibility in the choice of observables has allowed various extensions we mentioned above tailored to domain specific applications at hand [2,3,59].

By definition, DMD can extract spatially coherent structures and temporal pattern from data, which corresponds to modal properties such as mode shapes, natural frequencies and damping ratios, in vibrating structures. However to our knowledge it has not been widely employed in the field of structural dynamics. This gap in the literature is partly attributed to the strong dominance of principal component decomposition (POD) [60,61] and subspace-based SID techniques [31,62] among structural dynamics researchers and also to the requirement of high dimensional data (full state measurements) for DMD [2]. The requirement of full state measurements for the DMD is somewhat restrictive, limiting the methodology's application in fields with high dimensional data. In practice, for mechanical systems, responses can only be measured at specific strategic locations owing to limitations in the acquisition hardware, and internal full model operators are seldom available. Sparse system identification techniques such as blind source separation [34,35,63,64], sparse component analysis [65,66], empirical mode decomposition [67–69] and synchro-squeezed transform [70,71] have been effectively applied for modal identification of dynamical systems with limited measurements, in the context of structural health monitoring. However, incorporating these techniques in the framework of DMD is challenging and hence, researchers have taken inspiration from Taken's embedding theory [72] and proposed applying the DMD procedure on time-shifted coordinates [40,50,54–56]. These methods require accurate tuning of the time delays (or hyper-parameters), which is often problem-specific, and noise in the observed data may lead to erroneous results [40,73]. Recent works have proposed techniques to address these problems and the interested reader is referred to, e.g., [39,56,74,75] and the references therein for more details.

In the present study, for systems with a limited number of measurements a novel data-driven methodology called Wavelet-based Dynamic mode Decomposition (WDMD) is proposed. The proposed methodology builds on ioDMD and utilizes the wavelet decomposition of measured responses as observables, thereby enlarging the state dimensions. In other words, wavelet coefficients of the measured outputs serve as the pseudo-states of the dynamical system, and the DMD framework approximates a linear operator that advances the pseudo-states by a time step. The present approach can be thought of as a particular case of EDMD with a special choice of the observables. Hence, the present methodology can be applied to model dynamical systems such as a vibrating mechanical system, whose internal state vectors are not readily available, and only data from a few output locations are accessible, which is often the case in practice.

In the present context, data-driven modeling creates numerical models for capturing the input–output characteristics of the underlying structure. The advantage with such models is that it relies completely on measured responses, thereby circumventing the need for the knowledge of any underlying governing dynamics of the structure. In this paper, the data corresponds to time-domain samples of the input–output trajectories, and modeling equates to the best fit linear operator that advances the system states by a time step. In this paper, the data is fixed, only some outputs are observed and one cannot go back to re-query the

dynamics. The authors refer the reader to [74,76], which deals with the partial state observation where it is possible to re-query the system dynamics at each stage. For data-driven techniques that uses frequency domain samples, the authors refer the reader to [7,8,17,18,77–79] and the references therein.

The major contributions of this papers are as follows: First, a new data-driven modeling methodology (WDMD) is proposed that utilizes only the input–output trajectories of the system. To the authors' best knowledge, extending ioDMD's applicability through the use of wavelets has not yet been explored. The proposed methodology provides at least the same and in many cases better quality of the fit using only input–output trajectories, compared with the baseline approach, which has access to full state information. In addition, our present work provides a means to apply the DMD algorithm towards modal analysis and structural vibration of a mechanical system. Finally, these numerical results are complemented with experimental tests on a free–free aluminum cantilever beam, in which WDMD methodology is utilized to develop data-driven models from (noisy) real data.

The paper is structured as follows. First, a brief description of DMD, ioDMD, and EDMD are presented in Section 2. In Section 3, our work's major contribution, WDMD, is derived. The proposed methodology is demonstrated on data from a simulated finite element model of a cantilever beam in Section 4. In Section 5, experimental case studies are carried out on a free–free beam to demonstrate the efficiency and robustness of the WDMD in approximating practical mechanical systems. Conclusions and potential future directions are given in Section 6.

## 2. Background

### 2.1. Dynamic mode decomposition

In this section, a brief introduction to the classical dynamic mode decomposition (DMD) framework is provided. For details, we refer the reader to [1,3,80] and the references therein. Consider the system of time-invariant ordinary differential equations of the form

$$\dot{\mathbf{x}}(t) = f(\mathbf{x}(t)), \quad (1)$$

where  $\mathbf{x}(t) \in \mathbb{R}^N$  is the state vector and  $f : \mathbb{R}^N \rightarrow \mathbb{R}^N$  is a nonlinear map. Given the sampling times  $t_0, t_1, \dots, t_K$  (equally distanced), let  $\{\mathbf{x}(t_0), \mathbf{x}(t_1), \dots, \mathbf{x}(t_K)\}$  denote the samples of the state  $\mathbf{x}(t)$  of dynamical system Eq. (1). For this data, define two snapshot matrices  $\mathbf{X}_0$  and  $\mathbf{X}_1$  as

$$\mathbf{X}_0 = [\mathbf{x}(t_0) \quad \mathbf{x}(t_1) \quad \dots \quad \mathbf{x}(t_{K-1})] \in \mathbb{R}^{N \times K} \quad \text{and} \quad \mathbf{X}_1 = [\mathbf{x}(t_1) \quad \mathbf{x}(t_2) \quad \dots \quad \mathbf{x}(t_K)] \in \mathbb{R}^{N \times K}, \quad (2)$$

where  $\mathbf{X}_0$  denotes the snapshot matrix from  $t_0$  to  $t_{K-1}$  and  $\mathbf{X}_1 \in \mathbb{R}^{N \times K-1}$  from  $t_1$  to  $t_K$ , which advances the  $\mathbf{X}_0$  matrix by one time step. The most fundamental form of DMD aims to explain the snapshot data with a linear dynamical system of the form,

$$\mathbf{x}(t_{k+1}) \approx \mathbf{A}\mathbf{x}(t_k), \quad \text{for } k = 0, 1, 2, \dots, K-1, \text{ where } \mathbf{A} \in \mathbb{R}^{N \times N}. \quad (3)$$

In terms of  $\mathbf{X}_0$  and  $\mathbf{X}_1$ , the approximation in Eq. (3) can be written in the matrix form as

$$\mathbf{X}_1 \approx \mathbf{A}\mathbf{X}_0. \quad (4)$$

The DMD algorithm finds the best-fit solution  $\mathbf{A}$ , one that minimizes the least-squares distance in the Frobenius norm, i.e.,

$$\mathbf{A} = \arg \min_{\hat{\mathbf{A}} \in \mathbb{R}^{N \times N}} \|\mathbf{X}_1 - \hat{\mathbf{A}}\mathbf{X}_0\|_F. \quad (5)$$

The optimal solution  $\mathbf{A}$  in Eq. (5) is given by

$$\mathbf{A} = \mathbf{X}_1 \mathbf{X}_0^\dagger, \quad (6)$$

where  $\mathbf{X}_0^\dagger \in \mathbb{R}^{K \times N}$  denotes the Moore–Penrose inverse of  $\mathbf{X}_0 \in \mathbb{R}^{N \times K}$ . The practical issues in computing the  $\mathbf{A}$  matrix involves algebraic assumptions and singular value decomposition of the  $\mathbf{X}_0$  matrix, which are skipped here for brevity. Interested readers are directed to [3,80–83] for more rigorous discussion on practical algorithms and computational considerations.

### 2.2. input–output Dynamic mode decomposition (ioDMD)

The DMD method as described in the previous section can only be used for systems that evolve on their own, with no external input and for which all states are assumed to be measured. However, dynamical systems in practice have external inputs and the form as represented by Eq. (3) will not be sufficient to explain the dynamics [84]. This lead to the development of DMD with controls (DMDc) [53] by including measurements of a control input  $\mathbf{u}(t)$ . The input–output DMD is a further extension of the DMDc by incorporating the observed outputs [43,85]. The ioDMD framework constructs a reduced-order model directly from the observed input–output data and the full state vector  $\mathbf{x}(t)$ . The ioDMD framework models the dynamical systems of the form

$$\begin{aligned} \dot{\mathbf{x}}(t) &= f(\mathbf{x}(t), \mathbf{u}(t)), \\ \mathbf{y}(t) &= g(\mathbf{x}(t), \mathbf{u}(t)), \end{aligned} \quad (7)$$

where  $\mathbf{u}(t) \in \mathbb{R}^m$  denotes the inputs driving the system and  $\mathbf{y}(t) \in \mathbb{R}^d$  is the measured output.

The ioDMD method approximates the evolution of Eq. (7) with a linear dynamical system of the form

$$\begin{aligned}\mathbf{x}(t_{k+1}) &\approx \mathbf{Ax}(t_k) + \mathbf{Bu}(t_k), \\ \mathbf{y}(t_k) &\approx \mathbf{Cx}(t_k) + \mathbf{Du}(t_k),\end{aligned}\quad (8)$$

where  $\mathbf{A} \in \mathbb{R}^{N \times N}$ ,  $\mathbf{B} \in \mathbb{R}^{N \times m}$ ,  $\mathbf{C} \in \mathbb{R}^{d \times N}$ ,  $\mathbf{D} \in \mathbb{R}^{d \times m}$ . In addition to the state snapshots  $\mathbf{X}_0$  and  $\mathbf{X}_1$  in Eq. (2), define the input and output snapshot matrices as

$$\mathbf{U}_0 = [\mathbf{u}(t_0) \quad \mathbf{u}(t_1) \quad \dots \quad \mathbf{u}(t_{K-1})] \in \mathbb{R}^{m \times K} \text{ and } \mathbf{Y}_0 = [\mathbf{y}(t_0) \quad \mathbf{y}(t_1) \quad \dots \quad \mathbf{y}(t_{K-1})] \in \mathbb{R}^{d \times K}. \quad (9)$$

This would entail writing Eq. (8) in terms of its matrix counterpart as

$$\begin{bmatrix} \mathbf{X}_1 \\ \mathbf{Y}_0 \end{bmatrix} \approx \begin{bmatrix} \mathbf{A} & \mathbf{B} \\ \mathbf{C} & \mathbf{D} \end{bmatrix} \begin{bmatrix} \mathbf{X}_0 \\ \mathbf{U}_0 \end{bmatrix}. \quad (10)$$

Let

$$\mathbf{Y} = \begin{bmatrix} \mathbf{A} & \mathbf{B} \\ \mathbf{C} & \mathbf{D} \end{bmatrix} \in \mathbb{R}^{(N+d) \times (N+m)} \quad (11)$$

denote the optimal solution to Eq. (10). Similar to the original DMD framework, the ioDMD method finds the optimal solution  $\mathbf{Y}$  by solving a least-squares problem, namely

$$\mathbf{Y} = \underset{\hat{\mathbf{Y}} \in \mathbb{R}^{(N+d) \times (N+m)}}{\arg \min} \left\| \begin{bmatrix} \mathbf{X}_1 \\ \mathbf{Y}_0 \end{bmatrix} - \hat{\mathbf{Y}} \begin{bmatrix} \mathbf{X}_0 \\ \mathbf{U}_0 \end{bmatrix} \right\|_F. \quad (12)$$

The optimal  $\mathbf{Y}$  in ioDMD is given by

$$\mathbf{Y} = \begin{bmatrix} \mathbf{A} & \mathbf{B} \\ \mathbf{C} & \mathbf{D} \end{bmatrix} = \begin{bmatrix} \mathbf{X}_1 \\ \mathbf{Y}_0 \end{bmatrix} \begin{bmatrix} \mathbf{X}_0 \\ \mathbf{U}_0 \end{bmatrix}^\dagger. \quad (13)$$

Practical issues that arise in computing Eq. (6) arise here as well. Computing the pseudo-inverse in Eq. (13) often involves inverting small non-zero singular values, thereby leading to numerical instabilities. Therefore, in practice, singular values below a relative tolerance  $\beta \in \mathbb{R}^+$  are truncated during the pseudo-inverse computation or other regularization techniques could be employed. One can also perform model reduction on the state snapshot matrix  $\mathbf{X}$  to further reduce the state-space dimension of the output linear dynamical system. This is carried out by performing an additional SVD-based projection step before solving the least squares problem in Eq. (12). We refer the reader to [3,43] for details.

### 2.3. Extended DMD and the Koopman operator

Koopman theory [42] has received considerable attention recently due to the pioneering work of Mezić et al. [86]. It has been shown that the DMD algorithm is a special case of Koopman theory applied to linearly consistent data [41,86] and the DMD modes approximate the Koopman eigenvalues if the set of observable is sufficiently large (i.e., it spans the eigenvectors of the Koopman operator) and the data has to be sufficiently rich (i.e., it covers the dynamics of interest) [3,52].

In the case of a linear system with full measurements, linear observable or full state measurements are sufficient for the DMD algorithm to recover the dynamics of the underlying systems, as they span the eigenvectors of the Koopman operator. However, in the case of partially observed state measurement or non-linear systems, direct application of the DMD algorithm falls short of recovering the underlying dynamics. This observation has lead to the development of extended DMD (EDMD) by Williams et al. [52], which creates new observables,  $\varphi$ , from the state vector. To give context to the proposed algorithm, WDDMD, it is pertinent to introduce EDMD, and the present section serves to do so. The Koopman operator  $\mathcal{K}$  acts directly on observables  $\varphi$  rather than on state-space [42,52], i.e.,

$$\mathcal{K}\varphi \triangleq \varphi \circ \mathcal{F} \Rightarrow \mathcal{K}\varphi(\mathbf{x}(t_k)) = \varphi(\mathbf{x}(t_{k+1})), \quad (14)$$

where  $\mathcal{F} : \mathcal{M} \rightarrow \mathcal{M}$  is the evolution operator, and  $\circ$  denotes the composition operator. Intuitively, the linear Koopman operator takes a scalar function  $\varphi$  and returns a new function  $\mathcal{K}\varphi$  that predicts the value of  $\varphi$ , one step ahead in future. It is to be noted that the dynamical system defined by  $\mathcal{F}$  and the one defined by  $\mathcal{K}$  are two different parameterizations of the same fundamental behavior.

EDMD aims to approximate the Koopman operator using a suitable choice of dictionary of observables,  $\mathcal{D} = [\varphi_1, \varphi_2, \dots, \varphi_{N_K}]$ . The vector valued function  $\Phi : \mathcal{M} \rightarrow \mathbb{C}^{1 \times N_K}$ , where

$$\Phi(\mathbf{x}) = [\varphi_1(\mathbf{x}), \varphi_2(\mathbf{x}), \dots, \varphi_{N_K}(\mathbf{x})], \quad (15)$$

can now be defined for the snapshot of the system,  $\mathbf{x}(t_k)$ , and for  $\mathbf{z}(t_k) = \mathcal{F}(\mathbf{x}(t_k))$ . Then, one proceeds by defining two snapshot matrices using the samples  $\Phi(\mathbf{x}(t_k))$  and  $\Phi(\mathcal{F}(\mathbf{x}(t_k)))$  for  $k = 0, 1, \dots, K$  and solves a least-squares problem to form the best fit matrix  $\mathbf{K} \in \mathbb{R}^{N_K \times N_K}$ . The eigenvalues and eigenvectors of the finite dimensional representation  $\mathbf{K}$  are then used to compute an approximation to the Koopman modes and Koopman eigenfunctions. Thus, EDMD provides a mean to approximate the infinite dimensional Koopman operator and Koopman eigenfunctions through the selection of observables. For details, the reader is referred to [52].

## 2.4. Problem formulation

Consider an underlying dynamical system evolving in an  $N$ -dimensional state-space, i.e.,

$$\dot{\mathbf{x}}(t) = f(\mathbf{x}(t), \mathbf{u}(t)), \quad (16)$$

where  $\mathbf{x}(t) \in \mathbb{R}^N$  is the state,  $\mathbf{u}(t) \in \mathbb{R}^m$  is the input, and  $f : \mathbb{R}^N \rightarrow \mathbb{R}^N$  is a nonlinear mapping. Assume that, unlike in DMD or ioDMD, we do not have access to the full-state samples  $\mathbf{x}(t_k)$ . Instead, we have only access to a measurement vector (output)  $\mathbf{y}(t) \in \mathbb{R}^d$  via an observation (output) matrix  $\mathbf{C} \in \mathbb{R}^{d \times N}$ , i.e., we have access to the output

$$\mathbf{y}(t) = \mathbf{C}\mathbf{x}(t). \quad (17)$$

Using only these output trajectories and the excitation input applied to the system, the proposed Wavelet based DMD (WDMD) methodology creates a dynamical system to approximate the time evolution of the underlying system. The next section mathematically details the WDMD methodology.

## 3. Wavelet-based dynamic mode decomposition

The main idea behind the present methodology is to create observables using the stationary wavelet coefficients of all the available output measurements, and thereby to approximate the Koopman operator that advances these observables by a time step. Central to this idea is the wavelet transform. The next subsection, which mainly follows [87], presents a brief overview of the necessary background on wavelet transform. We refer the reader to [87–89] for details.

### 3.1. Maximal overlap discrete wavelet transform (MODWT)

The wavelet transform convolves a signal with a function called the mother wavelet, and the transform is computed across several scales representing different frequency bands for different segments of the signal. The wavelet transform provides a multi-resolution analysis (in contrast to the Fourier transform, which has a uniform time–frequency distribution.) The orthogonal wavelet decomposition of a signal  $y(t)$  is given by,

$$y(t) = \sum_j \sum_k w_k^j \psi_k^j, \quad (18)$$

with the wavelet coefficient  $w_k^j$  given by the inner product

$$w_k^j(y) = \left\langle y, \psi_k^j \right\rangle = \left\langle y(t), \frac{1}{2^{j/2}} \psi \left( \frac{t}{2^j} - k \right) \right\rangle = \frac{1}{2^{j/2}} \int_{-\infty}^{\infty} y(t) \psi^* \left( \frac{t}{2^j} - k \right) dt, \quad (19)$$

where the function  $\psi$  represents the mother wavelet,  $\psi_k^j = \frac{1}{2^{j/2}} \psi \left( \frac{t}{2^j} - k \right)$  is the scaled and translated mother wavelet, and  $(\cdot)^*$  denotes the complex conjugation. The transform is usually computed at discrete values in a grid corresponding to dyadic values of  $2^j$  and translations of  $k$ , where both  $j, k$  are integers, yielding the discrete wavelet transform (DWT).

In practice, successive high and low-pass filtering replaces the integration procedures in Eq. (19). This is followed by down-sampling at each level [87]. The coefficients resulting from these operations are called approximation and detail coefficients. The details of DWT implementation are not mentioned here for brevity, and interested readers are referred to seminal works such as [87]. Due to down sampling at each level, DWT wavelet coefficients do not have the property of time invariance.

The aforementioned issue can be addressed through a special type of wavelet transform known as the maximal overlap discrete wavelet transform (MODWT) [89]. MODWT has the advantage that it can eliminate down-sampling, thereby resulting in wavelet detail and scale coefficients at each level of the same length as the original time series, thereby facilitating a ready comparison between the series and its decomposition. Decomposing the time-series  $\{y(t_0), y(t_1), \dots, y(t_{K-1})\}$  using MODWT to  $J$  levels involves the application of  $J$  pairs of filters. The filtering procedure at  $j$ th level entails applying a high-pass filter ( $\tilde{h}_{j,l}^0$ ) known as wavelet filter, and low-pass filter ( $\tilde{g}_{j,l}^0$ ) known as scaling filter, where  $l = 1, 2, \dots, L_j$  is the length of the filter. This procedure yields a set of wavelet and scaling coefficients at each level  $j$  as

$$\tilde{W}_{j,t_k} = \sum_{l=0}^{K-1} \tilde{h}_{j,l} y(t_{k-l \bmod K}), \quad \tilde{V}_{j,t_k} = \sum_{l=0}^{K-1} \tilde{g}_{j,l} y(t_{k-l \bmod K}), \quad (20)$$

where  $\tilde{h}_{j,l}$  is  $\tilde{h}_{j,l}^0$  periodized to length  $K$  and  $\tilde{g}_{j,l}$  follows analogously using  $\tilde{g}_{j,l}^0$  values, and  $\bmod$  represents the modular operator; see [89] for details. The equivalent wavelet filter ( $\tilde{h}_{j,l}$ ) and scaling filter ( $\tilde{g}_{j,l}$ ) for the  $j$ th level are a set of scale-dependent localized differencing and averaging operators, respectively, and can be regarded as stretched versions of the base filter ( $j = 1$ ). The MODWT wavelet coefficients at each scale will have the same length as the original signal  $y(t)$  as seen from Eq. (20). Define the time-series vector

$$\mathbf{y} = [y(t_0), y(t_1), \dots, y(t_{K-1})]^T \in \mathbb{R}^K. \quad (21)$$

Then Eq. (20) can be expressed in matrix form as

$$\tilde{\mathbf{W}}_j = \tilde{\mathbf{W}}_j \mathbf{y} \quad \text{and} \quad \tilde{\mathbf{V}}_j = \tilde{\mathbf{V}}_j \mathbf{y}, \quad (22)$$

where  $\widetilde{\mathbf{W}}_j = [\widetilde{W}_{j,t_0}, \widetilde{W}_{j,t_1}, \dots, \widetilde{W}_{j,t_{K-1}}]^T \in \mathfrak{R}^K$  and  $\widetilde{\mathbf{V}}_j = [\widetilde{V}_{j,t_0}, \widetilde{V}_{j,t_1}, \dots, \widetilde{V}_{j,t_{K-1}}]^T \in \mathfrak{R}^K$  represent the  $j$ th level MODWT wavelet and scaling coefficients, respectively. The  $K \times K$  matrix  $\widetilde{\mathbf{W}}_j$  is defined as

$$\widetilde{\mathbf{W}}_j = \frac{1}{2^k} \begin{bmatrix} \widetilde{h}_{j,0} & \widetilde{h}_{j,K-1} & \widetilde{h}_{j,K-2} & \dots & \widetilde{h}_{j,3} & \widetilde{h}_{j,2} & \widetilde{h}_{j,1} \\ \widetilde{h}_{j,1} & \widetilde{h}_{j,0} & \widetilde{h}_{j,K-1} & \dots & \widetilde{h}_{j,4} & \widetilde{h}_{j,3} & \widetilde{h}_{j,2} \\ \widetilde{h}_{j,2} & \widetilde{h}_{j,1} & \widetilde{h}_{j,0} & \dots & \widetilde{h}_{j,5} & \widetilde{h}_{j,4} & \widetilde{h}_{j,3} \\ \vdots & \vdots & \vdots & \dots & \vdots & \vdots & \vdots \\ \widetilde{h}_{j,K-2} & \widetilde{h}_{j,K-3} & \widetilde{h}_{j,K-4} & \dots & \widetilde{h}_{j,1} & \widetilde{h}_{j,0} & \widetilde{h}_{j,K-1} \\ \widetilde{h}_{j,K-1} & \widetilde{h}_{j,K-2} & \widetilde{h}_{j,K-3} & \dots & \widetilde{h}_{j,2} & \widetilde{h}_{j,1} & \widetilde{h}_{j,0} \end{bmatrix}, \quad (23)$$

and the  $K \times K$  matrix  $\widetilde{\mathbf{V}}_j$  is defined analogously using  $\widetilde{g}_{j,l}$  values; see [89] for details. The original time series  $y$  can be recovered from its MODWT via

$$\mathbf{y} = \sum_{j=1}^J \widetilde{\mathbf{W}}_j^T \widetilde{\mathbf{W}}_j + \widetilde{\mathbf{V}}_j^T \widetilde{\mathbf{V}}_j = \sum_{j=1}^J \widetilde{\mathbf{D}}_j + \widetilde{\mathbf{S}}_j \quad \text{where} \quad \widetilde{\mathbf{D}}_j := \widetilde{\mathbf{W}}_j^T \widetilde{\mathbf{W}}_j \in \mathfrak{R}^K \quad \text{and} \quad \widetilde{\mathbf{S}}_j = \widetilde{\mathbf{V}}_j^T \widetilde{\mathbf{V}}_j \in \mathfrak{R}^K. \quad (24)$$

The last equality defines a MODWT-based multi-resolution analysis (MRA) of the original time series  $\mathbf{y}$  in terms of  $j$ th level MODWT detail coefficients  $\widetilde{\mathbf{D}}_j$  and  $J$ th level MODWT smooth coefficients  $\widetilde{\mathbf{S}}_j$ .

### 3.2. Main approach

As mentioned in Section 2.4, the output trajectories of the underlying system are measured and assuming that these trajectories are sampled at time instances  $t_0, t_1, \dots, t_K$ , yielding the measurement samples

$$\mathbf{y}(t_k) = \mathbf{C}\mathbf{x}(t_k), \quad \text{for } k = 0, 1, \dots, K-1. \quad (25)$$

Based on MODWT analysis of the previous section, our goal is now to create new auxiliary state variables (and an observation matrix) so that the new dynamics with the auxiliary state still corresponds to the true output samples in Eq. (25). Then we can apply the ioDMD using the trajectories of the original input and outputs, and the trajectories of the auxiliary states.

Towards this goal, let  $y_i(t)$ , for  $i = 1, 2, \dots, d$ , denote the  $i$ th component (row) of the measurement vector  $\mathbf{y}(t)$ , i.e.,  $y_i(t)$  is the  $i$ th output. Decompose  $y_i(t)$  using MODWT as in Eq. (24):

$$\mathbf{y}_i = \sum_{j=1}^J \widetilde{\mathbf{D}}_j^{(i)} + \widetilde{\mathbf{S}}_j^{(i)} \quad \text{where} \quad \mathbf{y}_i = [y_i(t_0), y_i(t_1), \dots, y_i(t_{K-1})]^T, \quad (26)$$

and  $\widetilde{\mathbf{D}}_j^{(i)} \in \mathfrak{R}^K$  and  $\widetilde{\mathbf{S}}_j^{(i)} \in \mathfrak{R}^K$  are the corresponding  $j$ th level detail and smooth coefficients corresponding to  $y_i(t)$ . Let  $\mathbf{e}_k \in \mathfrak{R}^K$  denote the  $k$ th canonical vector and  $\mathbf{e} = [1 \ 1 \ \dots \ 1]^T \in \mathfrak{R}^{J+1}$  denote the vector of ones. Then, using Eq. (26),  $y_i(t_k)$  (the  $(K+1)$ st row of  $\mathbf{y}_i = [y_i(t_0), y_i(t_1), \dots, y_i(t_{K-1})]^T$ ) can be written as

$$y_i(t_k) = \mathbf{e}_{k+1}^T \mathbf{y}_i = \sum_{j=1}^J \mathbf{e}_{k+1}^T \widetilde{\mathbf{D}}_j^{(i)} + \mathbf{e}_{k+1}^T \widetilde{\mathbf{S}}_j^{(i)} = \mathbf{e}^T \mathbf{w}_i(t_k) \quad (27)$$

where

$$\mathbf{w}_i(t_k) = \begin{bmatrix} \mathbf{e}_{k+1}^T \widetilde{\mathbf{D}}_1^{(i)} \\ \mathbf{e}_{k+1}^T \widetilde{\mathbf{D}}_2^{(i)} \\ \vdots \\ \mathbf{e}_{k+1}^T \widetilde{\mathbf{D}}_J^{(i)} \\ \mathbf{e}_{k+1}^T \widetilde{\mathbf{S}}_J^{(i)} \end{bmatrix} \in \mathfrak{R}^{J+1}. \quad (28)$$

Then, the full output vector at time  $t_k$ , i.e.,  $\mathbf{y}(t_k)$  in Eq. (25), can be rewritten as

$$\mathbf{y}(t_k) = \begin{bmatrix} y_1(t_k) \\ y_2(t_k) \\ \vdots \\ y_d(t_k) \end{bmatrix} = \begin{bmatrix} \mathbf{e}^T \mathbf{w}_1(t_k) \\ \mathbf{e}^T \mathbf{w}_2(t_k) \\ \vdots \\ \mathbf{e}^T \mathbf{w}_d(t_k) \end{bmatrix}. \quad (29)$$

Using the last formula, we define the new auxiliary state  $\mathbf{z}(t)$  and the observation matrix  $\mathbf{C}_w$

$$\mathbf{z}(t_k) = \begin{bmatrix} \mathbf{w}_1(t_k) \\ \mathbf{w}_2(t_k) \\ \vdots \\ \mathbf{w}_d(t_k) \end{bmatrix} \in \mathfrak{R}^{d(J+1)} \quad \text{and} \quad \mathbf{C}_w = \begin{bmatrix} \mathbf{e}^T & 0 & \dots & 0 & 0 \\ 0 & \mathbf{e}^T & \ddots & 0 & 0 \\ \vdots & \ddots & \ddots & \ddots & \vdots \\ 0 & 0 & \ddots & \mathbf{e}^T & 0 \\ 0 & 0 & \dots & 0 & \mathbf{e}^T \end{bmatrix} \in \mathfrak{R}^{d \times d(J+1)}, \quad (30)$$

so that

$$\mathbf{y}(t_k) = \mathbf{C}_w \mathbf{z}(t_k). \quad (31)$$

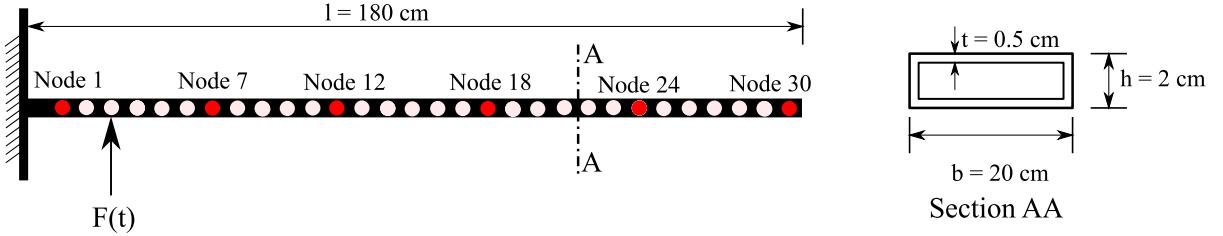


Fig. 1. Cantilever beam model used for the Finite Element simulations.

Note that the new auxiliary state variable  $\mathbf{z}(t)$  is composed of the wavelet coefficient observables and thus its samples encodes how the wavelet coefficient observables evolve over time. Moreover, with the observation matrix  $\mathbf{C}_w$ , the true output/measurement vector  $\mathbf{y}(t)$  is written in terms of the new state variable  $\mathbf{z}(t)$ .

Given only the output snapshots  $\mathbf{y}(t_k)$  in Eq. (25) of the underlying dynamical system, use Eq. (26)–Eq. (30) to construct the snapshot matrix  $\mathbf{Z}$  of the wavelet coefficient observables as

$$\mathbf{Z} = [\mathbf{z}(t_0) \ \mathbf{z}(t_1) \ \mathbf{z}(t_2) \ \dots \ \mathbf{z}(t_K)] \in \mathbb{R}^{d(J+1) \times (K+1)}. \quad (32)$$

Also construct the input snapshot matrix  $\mathbf{U}_0$  and  $\mathbf{Y}_0$

$$\mathbf{U}_0 = [\mathbf{u}(t_0) \ \mathbf{u}(t_1) \ \dots \ \mathbf{u}(t_{K-1})] \in \mathbb{R}^{M \times K} \text{ and } \mathbf{Y}_0 = [\mathbf{y}(t_0) \ \mathbf{y}(t_1) \ \dots \ \mathbf{y}(t_{K-1})] \in \mathbb{R}^{d \times K}. \quad (33)$$

Note that while the input snapshot matrix  $\mathbf{U}_0$  and the output snapshot matrix  $\mathbf{Y}_0$  in Eq. (33) correspond to the true inputs and outputs of the underlying dynamical system Eqs. (16) and (17), the state snapshot matrix  $\mathbf{Z}$  in Eq. (32) are obtained via the wavelet coefficient observables (as the original state measurements  $\mathbf{x}(t_k)$  are not available). Then, WDMD represents the snapshot triplets  $\mathbf{Z}, \mathbf{U}_0$  and  $\mathbf{Y}_0$  with the dynamical system

$$\mathbf{z}(t_{k+1}) \approx \mathbf{A}_w(t_k)\mathbf{z}(t_k) + \mathbf{B}_w\mathbf{u}(t_k), \quad \mathbf{y}(t_k) \approx \mathbf{C}_w\mathbf{z}(t_k) + \mathbf{D}_w\mathbf{u}(t_k). \quad (34)$$

This reformulation of the input/output data via wavelet coefficient observables to input/state/output data allows to apply ioDMD to construct the matrices  $\mathbf{A}_w$ ,  $\mathbf{B}_w$ ,  $\mathbf{C}_w$ , and  $\mathbf{D}_w$  via a least-squares fit as in Section 2.2. Towards this goal, define the two matrices

$$\mathbf{Z}_0 = [\mathbf{z}(t_0), \ \mathbf{z}(t_1), \ \dots, \ \mathbf{z}(t_{K-1})] \in \mathbb{R}^{d \cdot (J+1) \times K} \text{ and } \mathbf{Z}_1 = [\mathbf{z}(t_1), \ \mathbf{z}(t_2), \ \dots, \ \mathbf{z}(t_K)] \in \mathbb{R}^{d \cdot (J+1) \times K}. \quad (35)$$

Then, the dynamical system coefficients in Eq. (34) are given by

$$\begin{bmatrix} \mathbf{A}_w & \mathbf{B}_w \\ \mathbf{C}_w & \mathbf{D}_w \end{bmatrix} = \begin{bmatrix} \mathbf{Z}_1 \\ \mathbf{Y}_0 \end{bmatrix} \begin{bmatrix} \mathbf{Z}_0 \\ \mathbf{U}_0 \end{bmatrix}^\dagger. \quad (36)$$

A brief algorithmic sketch of WDMD is given in Algorithm 1.

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#### Algorithm 1 WDMD algorithm

**Input:** Output measurements  $\{\mathbf{y}(t_i)\} \in \mathbb{R}^d$  and input measurements  $\{\mathbf{u}(t_i)\} \in \mathbb{R}^m$  for  $i = 0, 1, \dots, K$ .

**Output:** State-space model:  $\mathbf{A}_w \in \mathbb{R}^{d \cdot (J+1) \times d \cdot (J+1)}$ ,  $\mathbf{B}_w \in \mathbb{R}^{d \cdot (J+1) \times m}$ ,  $\mathbf{C}_w \in \mathbb{R}^{d \times d \cdot (J+1)}$ , and  $\mathbf{D}_w \in \mathbb{R}^{d \times m}$ .

- 1: Using  $\{\mathbf{y}(t_i)\}$ , construct the wavelet observable snapshots  $\{\mathbf{z}(t_i)\}$  using Eqs. (26)–(30).
- 2: Form  $\mathbf{Z} = [\mathbf{z}(t_0) \ \mathbf{z}(t_1) \ \mathbf{z}(t_2) \ \dots \ \mathbf{z}(t_K)]$  as in Eq. (32)
- 3: Assemble  $\mathbf{Z}_0$  and  $\mathbf{Z}_1$  as in Eq. (35), and  $\mathbf{Y}_0$  and  $\mathbf{U}_0$  as in (33).
- 4: Compute the approximate discrete linear state-space matrices as in Eq. (36)

---

Given only the output samples, the present work's major contribution is to enlarge the original subspace via wavelet decomposition of the response measurement  $\mathbf{y}(t)$  and creating new states of the system using the wavelet coefficients. Therefore, the WDMD methodology can be considered a special case of EDMD with choice of observables in Eq. (15) resulting from the wavelet coefficients  $w_k^j(\mathbf{y}) = \langle \mathbf{y}, \psi_k^j \rangle$ . Thus, WDMD provides a set of basis functions to lift the output measurements to wavelet states, in a sense aiming to span the eigenvectors of the Koopman operator through ioDMD. Limitations will arise when there are fewer wavelet states, which will result from a combination of far fewer measurements alongside with smaller decomposition level  $J$ . Even though this issue can be circumvented by selecting a large enough decomposition level, the authors would like to note that the highest value of  $J$  is limited by the sampling frequency of the signal.

#### 4. A numerical case study using a finite element beam

Numerical simulations are carried out on a hollow cantilever beam model with the dimensions shown in Fig. 1. The beam under study is a finite element representation of an Euler–Bernoulli beam with 30 nodal points representing 60 degrees of freedom (DOF).

Taking the displacement and velocity of each DOF as the states yields a state-space representation in the first-order form

$$\dot{\mathbf{x}}(t) = \underbrace{\begin{bmatrix} \mathbf{0} \\ -\mathbf{M}^{-1}\mathbf{K} \\ -\mathbf{M}^{-1}\mathbf{G} \end{bmatrix}}_{:=\mathbf{A}} \mathbf{x}(t) + \underbrace{\begin{bmatrix} \mathbf{0} \\ -\mathbf{M}^{-1}\mathbf{F} \end{bmatrix}}_{:=\mathbf{B}} \mathbf{u}(t), \quad \mathbf{y}(t) = \mathbf{C}\mathbf{x}(t), \quad (37)$$

where  $\mathbf{M}, \mathbf{K}, \mathbf{G} \in \mathbb{R}^{60 \times 60}$  are, respectively, the mass, stiffness, and damping matrices and  $\mathbf{F} \in \mathbb{R}^{60 \times 1}$  is the loading vector;  $\mathbf{x} \in \mathbb{R}^{120 \times 1}$  is the state vector;  $\mathbf{u}(t) \in \mathbb{R}$  is the scalar input; and  $\mathbf{y} \in \mathbb{R}^d$  is the  $d$ -dimensional output vector. This yields the first-order state-space quantities  $\mathbf{A} \in \mathbb{R}^{120 \times 120}$ ,  $\mathbf{B} \in \mathbb{R}^{120}$ , and  $\mathbf{C} \in \mathbb{R}^{d \times 120}$ . The outputs, observed in  $\mathbf{y}$ , can be either the displacement or velocity of the observed nodal points. The choice of output will be further clarified below.

The proposed WDMD approach will be utilized to generate a single-input/multiple-output (SIMO), data-driven approximation to the beam model in Eq. (37) using *only* the simulated input–output response of the beam *without* access to its state-space matrices. This model will then be used to simulate the transient dynamic response of the structure to a given excitation (a testing signal) to illustrate the quality of the fit. In addition to this time-domain error measure, the input–output mapping of the data-driven model can also be assessed in the frequency domain by computing the frequency response function (FRF) of the learned model and comparing it with the original FRF. The FRF of the beam model Eq. (37), denoted by  $\mathcal{H}(\omega)$ , is given by

$$\mathcal{H}(\omega) = \mathbf{C}(\iota\omega\mathbf{I} - \mathbf{A})^{-1}\mathbf{B}, \quad (38)$$

where  $\iota^2 = -1$ . Let  $\tilde{\mathcal{H}}$  denote the FRF of the learned model and  $\tilde{\mathbf{y}}(t)$  the output of the learned. Then, the following two relative error metrics are defined to evaluate the quality of the fit,

$$\epsilon_{fd}^{rel} = \sqrt{\frac{\sum_{j=1}^{L_\omega} \|\mathcal{H}(\omega_j) - \tilde{\mathcal{H}}(\omega_j)\|_2^2}{\sum_{j=1}^{L_\omega} \|\mathcal{H}(\omega_j)\|_2^2}} \quad \text{and} \quad \epsilon_{td}^{rel} = \sqrt{\frac{\sum_{i=1}^K \|\mathbf{y}(t_i) - \tilde{\mathbf{y}}(t_i)\|_2^2}{\sum_{i=1}^K \|\mathbf{y}(t_i)\|_2^2}}, \quad (39)$$

where  $L_\omega$  and  $K$  are the number of frequency samples and time points respectively. While  $\epsilon_{fd}^{rel}$  is the relative error between the original FRF ( $\mathcal{H}(\omega)$ ) and the fitted FRF ( $\tilde{\mathcal{H}}(\omega)$ ),  $\epsilon_{td}^{rel}$  measures the relative error in time domain between the measured responses  $\mathbf{y}(t)$  and the predicted responses  $\tilde{\mathbf{y}}(t)$ .

In the present numerical case study, the FEM beam is excited using a chirp input over the frequency range 10–800 Hz. The responses are collected at a sampling frequency of 5000 Hz. The application of the ioDMD methodology, which assumes access to full state observation, for modeling the input–output response of the FEM beam, is demonstrated in Section 4.1. Next, in Section 4.2 we compare these results with WDMD. In Section 4.4 we present a brief comparative study between WDMD and Delay-DMD. As mentioned earlier, one can perform an additional model reduction via an SVD-based projection on the state data to further reduce the learned system dynamics [3,43]. In the present study, this additional step has yielded negligible changes to the final data-driven model and thus is skipped in all the results.

#### 4.1. Data-driven modeling using ioDMD

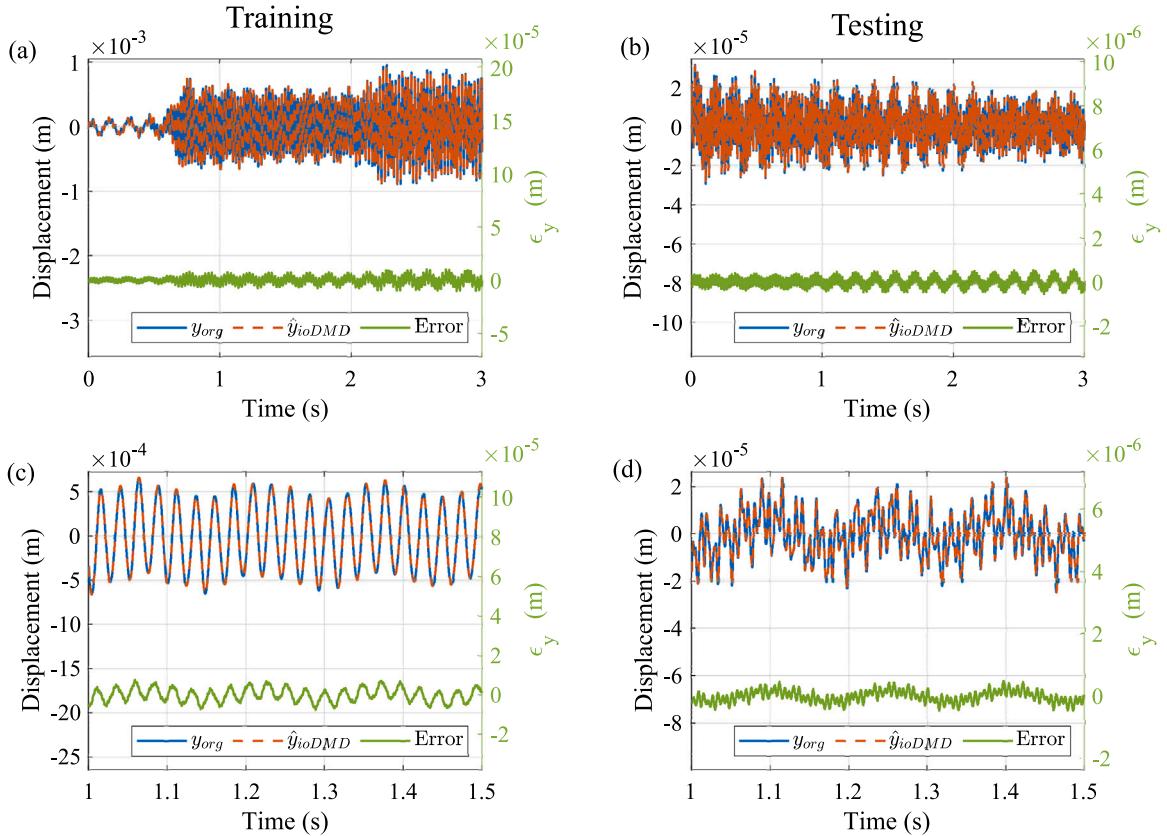
As discussed in Section 2.2, the ioDMD methodology assumes knowledge about the system’s full internal states  $\mathbf{x}(t)$ . Hence, the ioDMD is ideally suited towards gray box modeling wherein the internal states of the system are also sampled. For the beam’s finite element model, the internal states represent the displacement and velocity at each degree of freedom. The training package provided to the algorithm consists of: (i) the input forcing signal used to excite the structure (chirp signal), (ii) the internal state measurements, and (iii) the measured output responses. In the current example, the ioDMD has access to all the internal states of the system and the output is assumed to be measured at the 6 nodal points shown in Fig. 1. The measured displacements at nodes 1, 7, 12, 18, 24, and 30 are designated as the output responses in the present section. From the provided training package, the ioDMD algorithm, as presented in Section 2.2, generates a linear discrete dynamical system of the form,

$$\begin{aligned} \mathbf{x}(t_{k+1}) &= \mathbf{A}\mathbf{x}(t_k) + \mathbf{B}\mathbf{u}(t_k), \\ \mathbf{y}(t_k) &= \mathbf{C}\mathbf{x}(t_k) + \mathbf{D}\mathbf{u}(t_k), \end{aligned} \quad (40)$$

to approximate the original beam dynamics in Eq. (37). The singular value truncation tolerance in the computation of the pseudoinverse in Eq. (13) is set to  $\beta = 10^{-12}$ . Since no model reduction step is applied to further reduce the system dimension, the learned model’s state dimension is equal to the total number of degrees of freedom in the finite element model, i.e., 120. Since, the output is measured at 6 nodal points, the SIMO ioDMD state-space model in Eq. (40) has 120 internal states, single input, and six output, and thus the state-space matrices are  $\mathbf{A} \in \mathbb{R}^{120 \times 120}$ ,  $\mathbf{B} \in \mathbb{R}^{120 \times 1}$ ,  $\mathbf{C} \in \mathbb{R}^{6 \times 120}$ , and  $\mathbf{D} \in \mathbb{R}^{6 \times 1}$ .

##### 4.1.1. ioDMD model training and testing results

The results of modeling the dynamic response of the FEM beam using ioDMD are summarized in Fig. 2. The data-driven ioDMD model is excited using the same chirp signal used for training the model. For demonstration purposes, among the six outputs, the predicted response output at node 18 ( $\hat{y}$ ) is compared with the measured output from the FEM simulations ( $y$ ) and is shown in Fig. 2(a). The low value of the time domain error ( $\epsilon_y = y - \hat{y}$ ), shown in green, in Fig. 2(a) demonstrates the good quality of the fit. The relative error of  $\epsilon_{td}^{rel} = 2.3 \times 10^{-2}$  further substantiates the good quality of the fit across all the 6 outputs in the time domain. For validation purposes, a sine burst at 165.1 Hz is used to excite the ioDMD model and quality of the fit analyzed. The Fig. 2(b)



**Fig. 2.** (a) Comparison of the predicted response and the original response measured at node 18 when excited with the same training signal (chirp); (b) Comparison of the predicted response and the original response measured at node 18 when excited with a sine burst at 165 Hz (testing data); (c) Zoomed up version of (a) demonstrating a high-fidelity approximation in the training phase (d) Zoomed up version of (b) demonstrating a high-fidelity approximation in the testing phase.

contrasts the simulated response from the ioDMD methodology with the original response measurement from node 18 in the testing case. The low value of the error plot in Fig. 2(b) clearly illustrates the validity of the model over the frequency ranges of interest. Fig. 2(c) and Fig. 2(d) presents zoomed versions of the training and testing case respectively. The relative time domain error for ioDMD is  $e_{td}^{rel} = 1.62 \times 10^{-2}$  for the testing case.

It is straightforward to recover the dynamic modes of the system under consideration using the developed state-space model. The finite element model is setup in such a way that the dynamic modes of the beam corresponds to the modes of vibration of the system [16]. The recovered modes ( $\phi_{ioDMD}$ ), as shown in Fig. 3(a), closely resemble the modes of vibration of a cantilever beam ( $\phi_{FEM}$ ). The quality of the modes recovered using the ioDMD methodology is evaluated using the model assurance criteria (MAC) [90]. If individual columns of  $\phi_{ioDMD}$ , representing the DMD modes, are a close match with that of  $\phi_{FEM}$ , then the MAC value will be close to 1. The value of 1 in the diagonal term in Fig. 3(b) shows that the recovered DMD correlates well with the actual modes of vibration of the system. The zeros in the off-diagonal position further validate the orthogonality of the DMD modes (also a property of the physical modes), thus further demonstrating the efficacy of the ioDMD model in accurately capturing the hidden dynamics of the system under consideration.

#### 4.2. Data-driven modeling using WDMD

We now apply the WDMD methodology to model the input–output dynamic responses of the simulated beam. WDMD is used to obtain a data-driven model, using the snapshots matrices of only the measured outputs at  $d = 6$  locations and the chirp input, recorded in training phase. It is important to note that WDMD develops a SIMO, data-driven, state-space model by *only* utilizing the input–output trajectories of the measured nodal points, thus circumventing the restrictive assumption to require the samples of all the latent states of the system. It will be shown in later sections that WDMD yields high-fidelity approximates even with a small number of outputs and the quality of the fit further improves with an increase in number of measured outputs. The parameters controlling the WDMD algorithm are (i) the type of wavelet and (ii) the level of wavelet decomposition. In the current study, the Haar wavelet [87] is selected as the default setting throughout and the level of decomposition in this section is  $J = 13$ . Although in

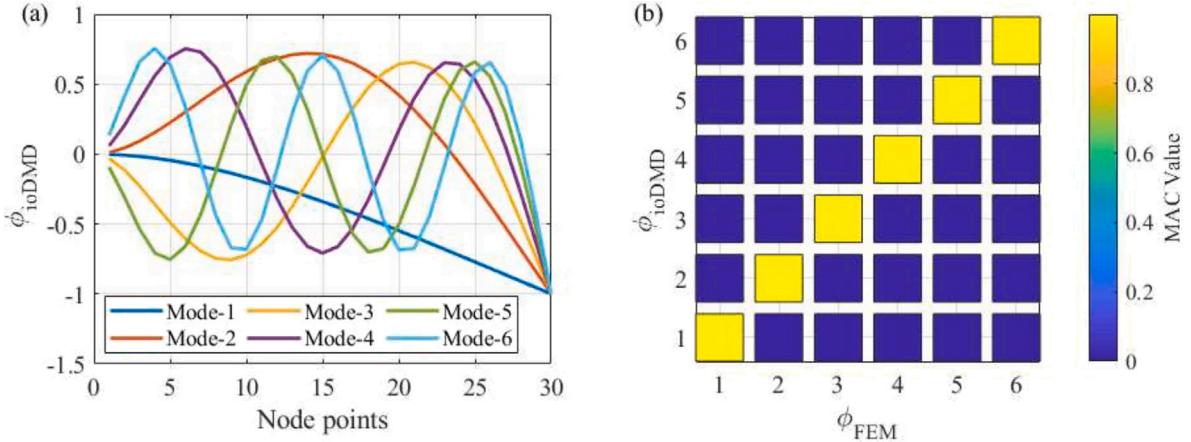


Fig. 3. (a) Mode shapes extracted by ioDMD (b) Comparison of the ioDMD modeshapes with the analytical mode shapes using modal assurance criterior (MAC).

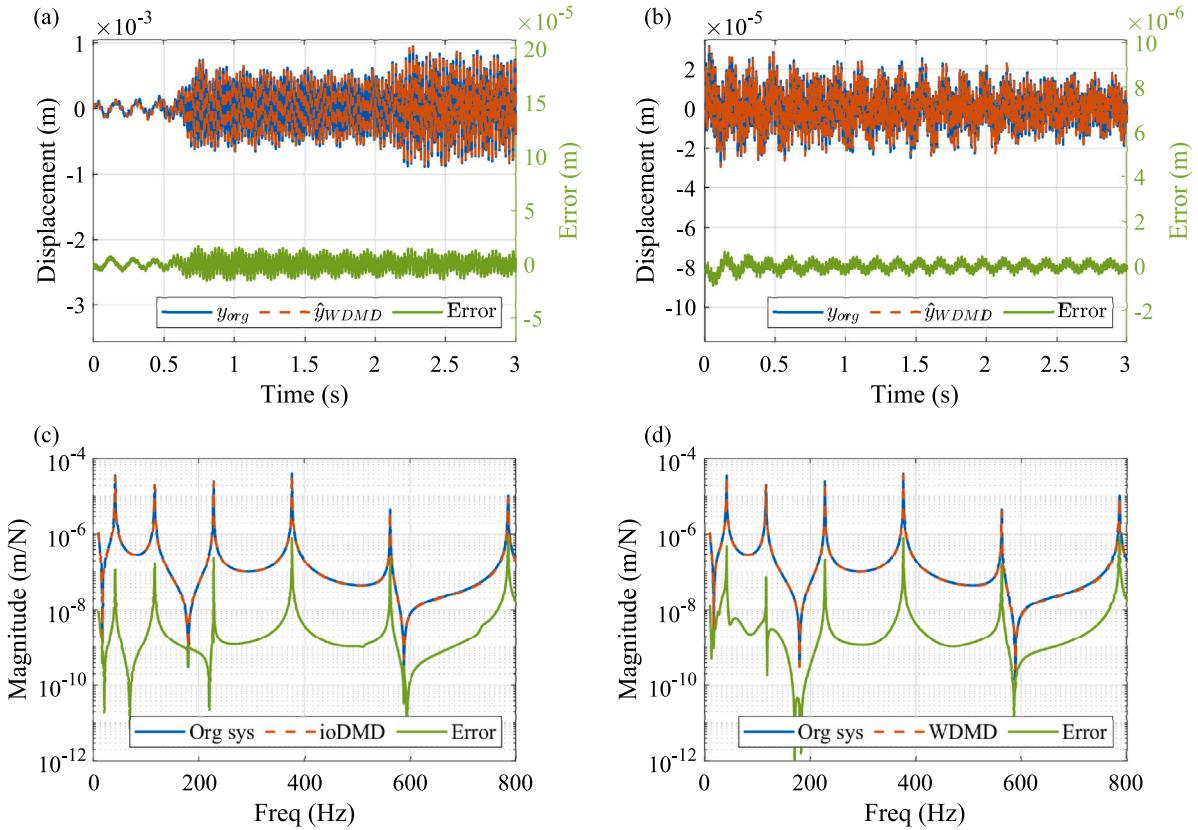


Fig. 4. (a) Comparison of the predicted response using WDMD and the original response measured at node 18 when excited with the training input, plotted alongside with the error in green; (b) Comparison of the predicted response using WDMD and the original response measured at node 18 when excited with the sine burst input at 165.1 Hz (testing phase), plotted alongside with the error in green; (c) Comparison of the magnitude of analytical and predicted FRF at node 18 using ioDMD alongside with error magnitudes; (d) Comparison of the magnitude of analytical and predicted FRF at node 18 using WDMD alongside with error magnitudes.

the current study the level of decomposition is set at  $J = 13$ , if needed one can use concepts such as hyper-parameter tuning based on k-fold cross validation, to select a more suitable  $J$ . As in the ioDMD case, the singular value truncation tolerance in computing the pseudoinverse is set to  $\beta = 10^{-12}$ . Based on these parameters, the number of auxiliary states in the resulting WDMD model in Eq. (34) is given by  $d \times (J + 1) = 84$ . Finally, this results in a state-space matrices with the following dimensions  $\mathbf{A}_w \in \mathbb{R}^{84 \times 84}$ ,  $\mathbf{B}_w \in \mathbb{R}^{84 \times 1}$ ,  $\mathbf{C}_w \in \mathbb{R}^{6 \times 84}$ , and  $\mathbf{D}_w \in \mathbb{R}^{6 \times 1}$ .

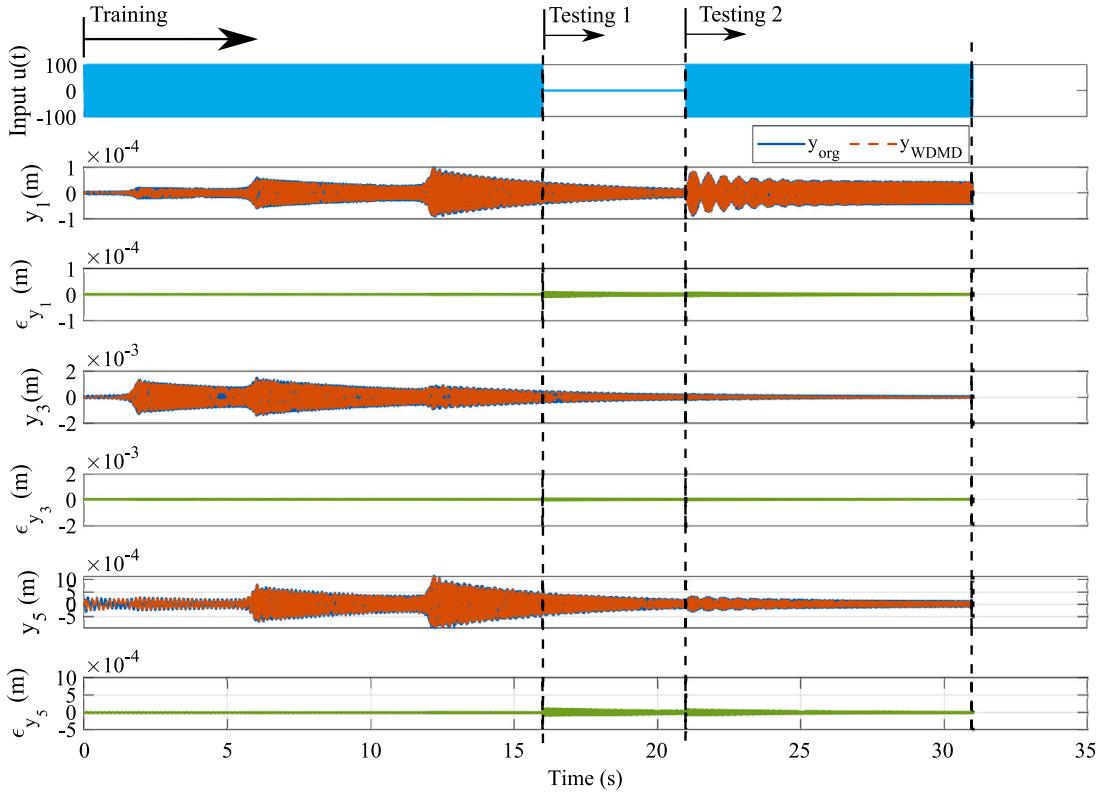


Fig. 5. Training phase followed by testing phases, comparing the predicted responses from WDMD model with the FEM simulation results.

#### 4.2.1. WDMD model training and testing results

The results of modeling the dynamic response of the FEM beam using WDMD are summarized in Fig. 4. For a first comparison, the data-driven model produced by WDMD is used to reproduce the behavior of the system during the training phase. To be consistent, we excite the WDMD model with the same training (chirp) and testing signal (sine burst) as in the ioDMD case. Fig. 4(a) shows the predicted response at node 18 alongside with the measured output from the FEM simulations, illustrating a high-fidelity match. The low value of the time domain error (green) in Fig. 4(a) further validates the good quality of the fit. The relative time-domain error of  $\epsilon_{td}^{rel} = 1.59 \times 10^{-2}$  across the 6 predicted response illustrates a better performance over ioDMD in this case. The sine burst at 165.1 Hz excites the SIMO WDMD model and the predicted response at node 18 is compared with that of FEM simulation results in Fig. 4(b). The testing phase results in a relative error of  $\epsilon_{td}^{rel} = 7.84 \times 10^{-3}$ .

To better illustrate the frequency domain performance, Fig. 4(c) and Fig. 4(d) depict, respectively, the magnitude of the predicted FRF ( $\tilde{H}_{iodmd}(\omega)$ ) due to ioDMD and predicted FRF ( $\tilde{H}_{wdmd}(\omega)$ ) due to WDMD, as compared to the original FRF ( $H(\omega)$ ) measured at node 18. While ioDMD results in a frequency domain relative error of  $\epsilon_{fd}^{rel} = 1.51 \times 10^{-2}$ , WDMD results in a slightly higher error value of  $\epsilon_{fd}^{rel} = 1.63 \times 10^{-2}$ . Nevertheless, both WDMD and ioDMD demonstrates excellent capability to capture the frequency domain characteristics of the system. And more importantly WDMD achieves this accuracy by measuring only 6 of the state variables out of the total 120.

To further test the capabilities of the WDMD model, two different testing phases are performed. The first test (Test 1) consists of a time interval with no excitation, thereby allowing the system to be driven by the initial conditions at the end of the training phase. The second test (Test 2) consists of a sine burst at 230.4 Hz. It is pertinent to observe that at no point during the beginning of a phase, the input conditions are corrected. This is particularly challenging for Test 1 where there is no input and thus small deviations in initial conditions can result in high errors. Fig. 5 shows 3 out of the 6 predicted responses alongside with the error between the WDMD model and the original FEM model. WDMD produces a high-quality fit for the all phases of these tests as can be seen from the low value of the errors, thus illustrating the efficacy of the algorithm.

Similar to the ioDMD case, the quality of the WDMD modes ( $\phi_{WDMD}$ ) and their agreement to the physical modes of the beam ( $\phi_{FEM}$ ) can be examined by using the MAC plots as shown in Fig. 6, where  $d$  represents the number of outputs measured. The quality of the extracted dynamic modes improves with the increase in total number of outputs measured as seen from Fig. 6. Nevertheless, even with a small number of measured output ( $d = 6$ ), WDMD resulted in a data-driven model that was able to meaningfully extract modal characteristics of the leading six modes as seen from the diagonal terms in Fig. 6(a). At  $d = 10$ , we see that WDMD results almost converge to the ioDMD MAC plots.

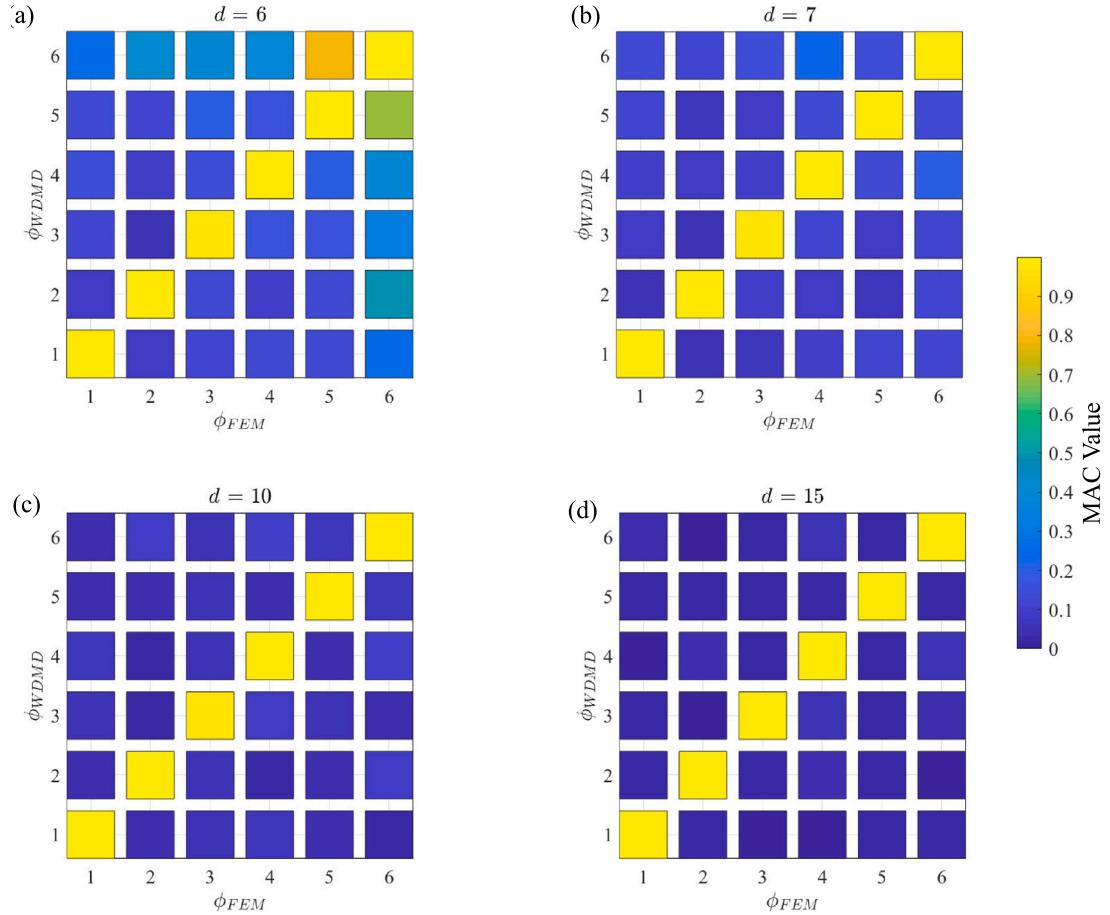


Fig. 6. MAC comparison plots for WDMD for (a)  $d = 6$ ; (b)  $d = 7$ ; (c)  $d = 10$ ; (d)  $d = 15$ .

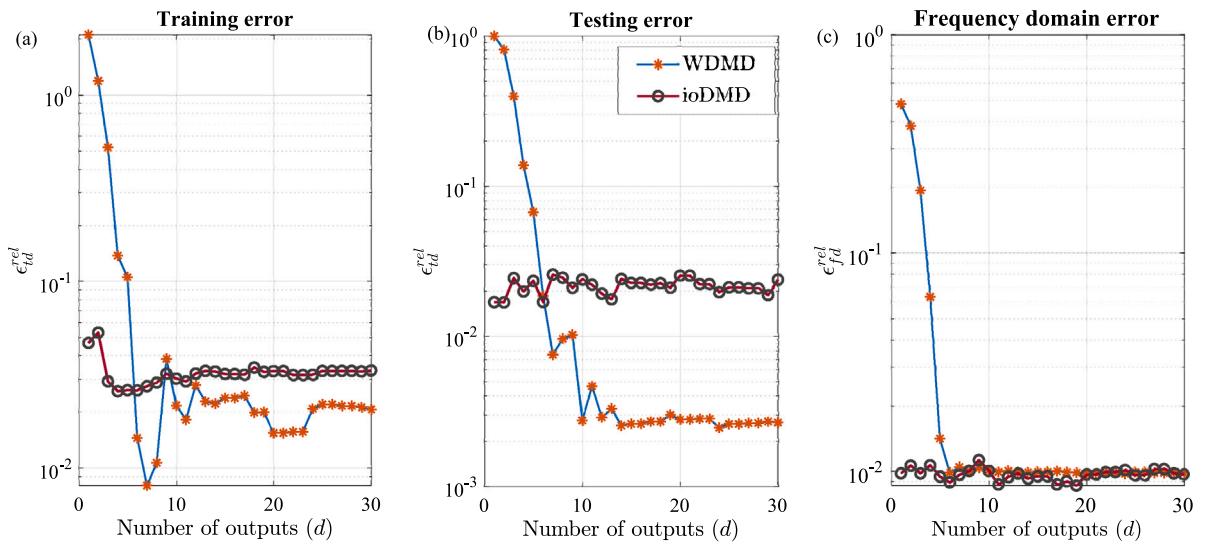
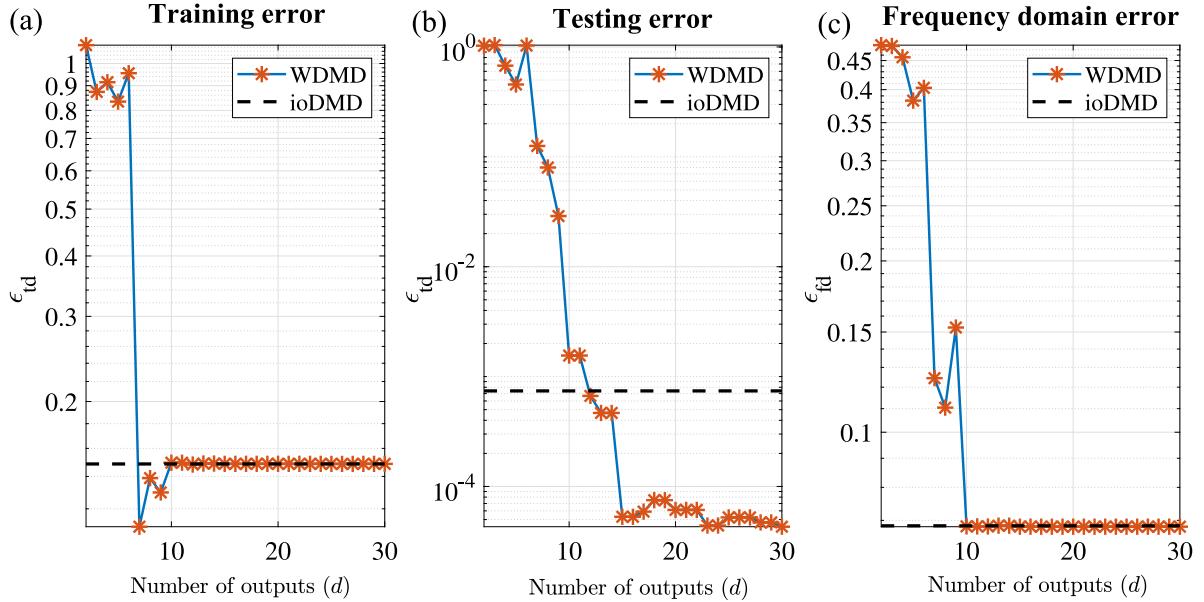


Fig. 7. Error convergence study results for the SIMO case: (a) Relative time domain error for training phase; (b) Relative time domain error for testing phase; (c) Relative frequency domain error.



**Fig. 8.** Error convergence study results for the MIMO case: (a) Relative time domain error for training phase; (b) Relative time domain error for testing phase; (c) Relative frequency domain error.

Since WDDMD only relies on input–output trajectories at the observed nodes, the major factor affecting the WDDMD methodology’s efficacy is the total number of outputs measured across the system. This necessitates an error convergence study in the time domain as well as in the frequency domain. By increasing the number of outputs measured, the quality of the fit improves as seen from Fig. 7. The figure shows the relative error as a function of the total number of measured outputs ( $d$ ). The figure also provides the ioDMD model error values for comparison purposes. Even with fewer measurements (as few as 6), for this example, the WDDMD methodology outperforms the ioDMD methodology. This figure demonstrates the advantage of applying the WDDMD in the practical situation wherein only a handful of the output trajectories can be measured. The same is true for the frequency domain representation. The relative error,  $\epsilon_{fd}^{rel}$  also drops as a function of the number of measurements available but eventually converges to the ioDMD model error of around 0.015.

#### 4.3. Results for the multiple input case - WDDMD

In this section, a multiple-input multiple-output (MIMO), state-space model using WDDMD is developed. Towards this goal, the FEM beam is subjected to uncorrelated input excitations at node 3 and node 17, thereby simulating multiple (two) input excitations. Similar to the SIMO case, WDDMD builds a data-driven model using measured outputs at selected nodal points and chirp inputs that are used for excitation, resulting in a MIMO learned model as in Eq. (34). WDDMD uses  $J = 13$  as before. Similar to the SIMO case, error convergence studies for the training and testing cases are performed. Fig. 8(a) and Fig. 8(b) shows error convergence plots for the training and testing case respectively as the number of outputs change. The WDDMD model error converges towards the full ioDMD baseline error for the training case, when the number of outputs ( $d$ ) measured are greater than 11. However for the testing case with  $d > 11$ , the WDDMD results in a lower testing error compared to the ioDMD model. These results follow the similar pattern to those of the SISO case. The smaller error for WDDMD in the testing case for this specific testing input might be due to the frequency content of the signal. Fig. 8 depicts the error in the frequency domain. Similar to the time domain error, there is no noticeable reduction in the error beyond  $d = 10$  and around this value the WDDMD error converges to the ioDMD model error. It is important to emphasize that WDDMD provides comparable results to ioDMD (and better in the time-domain testing case for this example) with a much smaller number of observed state. In this example, there are a total of 120 state variables with WDDMD observing only 10 of them (less than 10% of the total). Thus, WDDMD is able to match the full-state observation accurately.

#### 4.4. Comparison with the Delay-DMD

In this section, WDDMD is compared with Delay-DMD. Delay-DMD can be thought of as a special case of EDMD with the observable vector in Eq. (15) composed of the time-delayed versions of the measurements as,  $\Phi(\mathbf{x}_k) = [\mathbf{x}(t_k), \mathbf{x}(t_{k-\delta}), \dots, \mathbf{x}(t_{k-\delta\tau})]$ , where  $k = 1, 2, \dots, K - \delta\tau$  represent the snapshot indices. The integer  $\delta$  and  $\tau$  represent the lag-time and the embedding dimension, respectively. As with any algorithm, the performance of the Delay-DMD depends on various parameter choices, such as the lagtime  $\delta$  and the embedding dimension  $\tau$  that are often problem-specific [40,91]. Discussion regarding the parameter choices and embedding

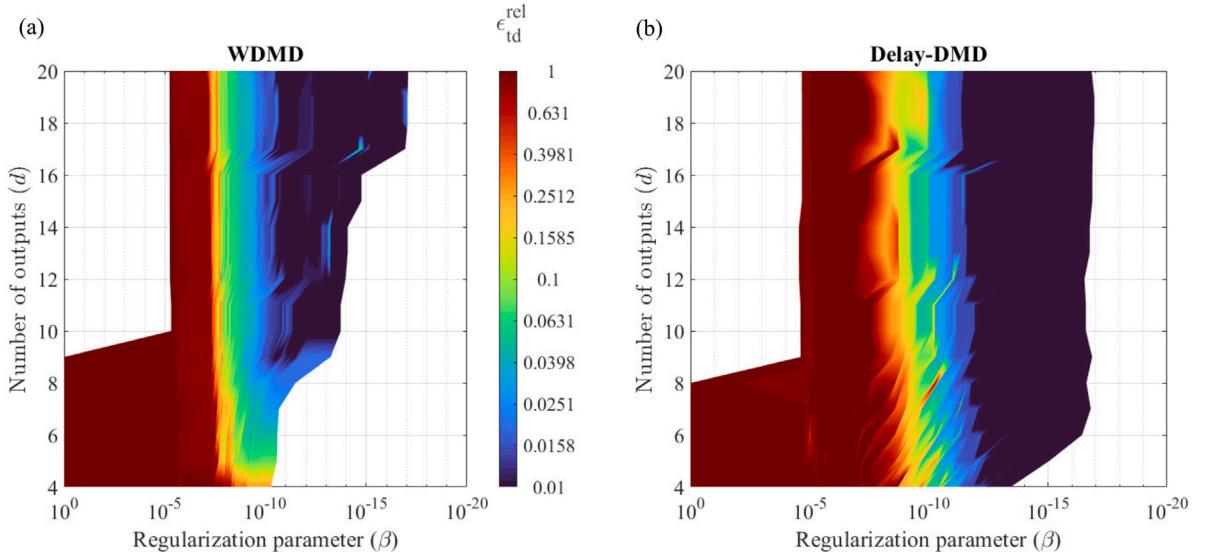


Fig. 9. Comparison of WDMD with Delay-DMD for the noise-free data using the  $\epsilon_{td}^{rel}$  measure as  $\beta$  and  $d$  vary.

dimensions are beyond the scope of the present study. For comparison purposes with WDMD,  $\delta$  is chosen as 1 and the embedding dimension is varied on a per case basis [3,40,91].

The present comparative study is conducted on the FEM beam model described in Section 4 with the same training and testing cases. As discussed in Section 4, the performance WDMD depends on the number of available measurements and the decomposition level. Thus, the number of available measurements is varied as one of the parameters.

The input-output trajectories of the FEM beam model are utilized by WDMD and Delay-DMD towards building a SIMO, data-driven, state-space model. For comparison purposes, both WDMD and Delay-DMD model are excited with the same chirp signal to reproduce the system's behavior during the training phase and the quality of the fit is assessed. Since both of these methods utilize only the measured input-output trajectories, the quality of the fit depends on the total number of measured responses,  $d$ . While WDMD results in a state-space model order of dimension  $d(J + 1)$ , Delay-DMD results in a model order of  $d \times \tau$ . Thus, Delay-DMD can lead to a bigger observable space even with a small number of measured outputs if the embedding dimension  $\tau$  is large enough, which lends Delay-DMD an advantage compared to WDMD. By introducing additional lag terms in the state-space, Delay-DMD can construct models with enhanced levels of complexity, for cases with a handful of measured outputs [3,40,91]. In the case of WDMD, this arbitrary enhancing is not possible, as the level of decomposition  $J$  is limited by the sampling frequency of the signal.

As explained in Section 2.2, apart from the number of responses measured, the performance of the algorithm also depends on the regularization parameter  $\beta$ . Therefore, for every training data set (i.e., for each value of  $d$ ), the parameter  $\beta$  is varied in both WDMD and Delay-DMD and the quality of the fit evaluated using  $\epsilon_{td}^{rel}$ . Therefore, for both WDMD and Delay-DMD the relative error  $\epsilon_{td}^{rel}$  is plotted in the form of surface contours with  $d$  and  $\beta$  being the two axes, as shown in Fig. 9(a) and Fig. 9(b), respectively.

In Figs. 9(a) and 9(b), three distinct regions are observed: (i)  $\beta > 10^{-8}$ , (ii)  $10^{-8} > \beta > 10^{-12}$ , and (iii)  $\beta < 10^{-12}$ . For the first region, both the training and testing errors are large for both methodologies, and this is attributed to the higher value of the regularization parameter, thus leading to an oversimplified model with significant singular values being truncated. However, in the second region, both methodologies demonstrate better performance, with WDMD having lower training and testing error compared to Delay-DMD. Finally, in the third region, Delay-DMD shows lower training error compared to the WDMD.

For most practical situations, the signal obtained from the sensors will be corrupted with noise. This warrants repeating the same set of simulations in the presence of added noise. Towards this goal, simulations are realized to study the performance of both methodologies in the presence of added noise. Zero-mean Gaussian white noise with amplitude corresponding to 0.5% of the measured signal is artificially added to all the outputs recorded from the FEM simulations and both methods are repeated. As expected, both methodologies perform poorly for  $\beta$  greater than  $10^{-5}$  as seen in the surface plots in Fig. 10. However, it is observed from Figs. 10(a) and 10(b) that for lower values of regularization parameter the training errors in WDMD algorithm are orders of magnitude smaller than Delay-DMD. We point out that prior to creating Fig. 9, an error convergence study was conducted with the varying  $\tau$  to select the (near-)optimal  $\tau$  value for Delay-DMD. The  $\tau$  value that resulted in the lowest relative error was selected and the comparison study with WDMD was done, thereby producing Fig. 9; thus Fig. 9 uses the best  $\tau$  for Delay-DMD. However for the noisy case in Fig. 10, in order to have a fair comparison with WDMD algorithm (whose  $J$  value was not changed between Figs. 9 and 10), we used the same  $\tau$  that gave the lowest relative error in the previous case. Thus Fig. 10 uses the same value of  $\tau$  as that of Fig. 9.

However, by no means this one numerical example claims to show that in the case of noisy data WDMD performs better in general. Authors acknowledge the fact that the issues observed with Delay-DMD in this one specific example may be resolved by

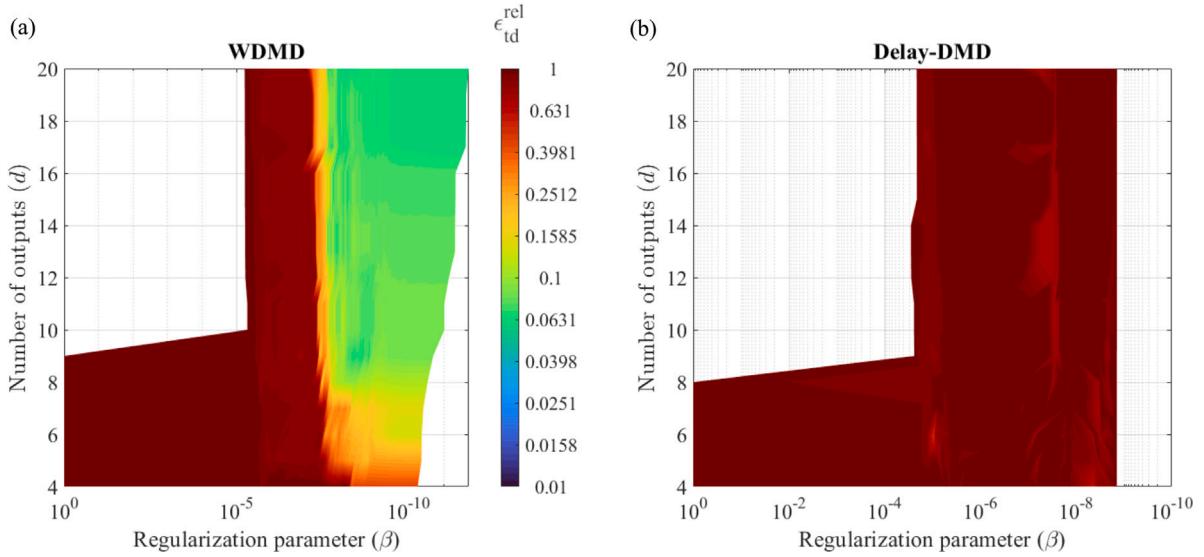


Fig. 10. Comparison of WDMD with Delay-DMD for the 0.5% additive noise case using the  $\epsilon_{td}^{rel}$  measure as  $\beta$  and  $d$  vary.

proper tuning of hyper-parameters, even though tuning these parameters for every possible case of noise could be challenging in practice [39,40]. The main goal of this numerical study was simply to see how WDMD might behave under noise if it was tuned, i.e., the level of decomposition  $J$ , for the noise-free data. It is possible that the smoothing operation inherent to the wavelet observables used in WDMD might naturally help with the noisy data. However, a detailed theoretical analysis of WDMD for the noisy case is beyond the scope of this paper and will be done in a future work.

## 5. Experimental study

We now present an experimental case study to validate the efficacy of the WDMD in modeling the dynamical response of a beam excited by an external forcing. The experimental set up used to measure the time domain response of the beam is depicted in Fig. 11. A 30 in. long aluminum beam with a rectangular cross-section of 1.5 in.  $\times$  0.1 in. (bxh) has been selected for this study. free-free boundary conditions are approximated by suspending the beam under test with fishing line wires. Two Macro Fiber Composites (MFCs), model number 29K06-005B, are bonded to either end of the beam for excitation purposes. The MFCs are actuated by supplying a Matlab generated signal delivered using an NI DAQ, and amplified through a power amplifier (Trek PZD350A-2-L). A scanning laser doppler vibrometer (SLDV), Polytec PSV-400, is used to measure the beam's dynamic response when excited with the MFC's. In the present set of experiments, 67 equally spaced scanning points are defined along the beam's length. The SLDV measures the velocity response of all the scanning points in the beam. The whole assembly has been placed on top of a Newport ST series smart table to isolate the effects of ground vibrations and other random excitations.

Using this setup, two sets of experiments are realized: (i) Single-input multiple-output (SIMO) and (ii) Multi-input multi-output (MIMO). Similar to the finite element simulations, the beam under study is excited using two sets of inputs for both of these cases: (i) Chirp signal over the frequency range 100 - 500 Hz to train the algorithm, and (ii) Sine burst to validate the model. The SLDV measures the output response (velocity) at a sampling rate of 5000 Hz from multiple locations along the beam. Measurement locations are densely selected to have enough data to study the effect of number of measurement points on the quality of the fit. In this experimental case study, the input corresponds to the voltage supplied to the MFC, while the output to the measured velocity responses.

### 5.1. Data-driven SIMO model

In this section, a SIMO, data-driven, state-space model is developed using WDMD based on the measured responses along the beam, valid over the frequency range of 100 to 500 Hz. The WDMD methodology utilizes the measured the velocity responses at 10 equidistant points along the beam and chirp input voltage supplied to the MFCs for building the data-driven SIMO model. It is pertinent to note that, although we measured velocity at 66 scanning points in the beam, we utilize only 10 output responses to develop the data-driven model. The level of wavelet decomposition ( $J$ ) is set as  $J = 13$ . Hence, WDMD outputs a linear discrete state-space form with the following dimensions:  $\mathbf{A}_w \in \mathbb{R}^{140 \times 140}$ ,  $\mathbf{B}_w \in \mathbb{R}^{140 \times 1}$ ,  $\mathbf{C}_w \in \mathbb{R}^{10 \times 140}$ , and  $\mathbf{D}_w \in \mathbb{R}^{10 \times 1}$ . The singular value truncation tolerance  $\beta$  is set to  $\beta = 10^{-12}$ .

Once the data-driven, SIMO, state-space model is developed, the behavior of the free-free beam during the training phase is reproduced using the recorded chirp input. For demonstration purpose, the predicted response (dashed orange line) at one of the

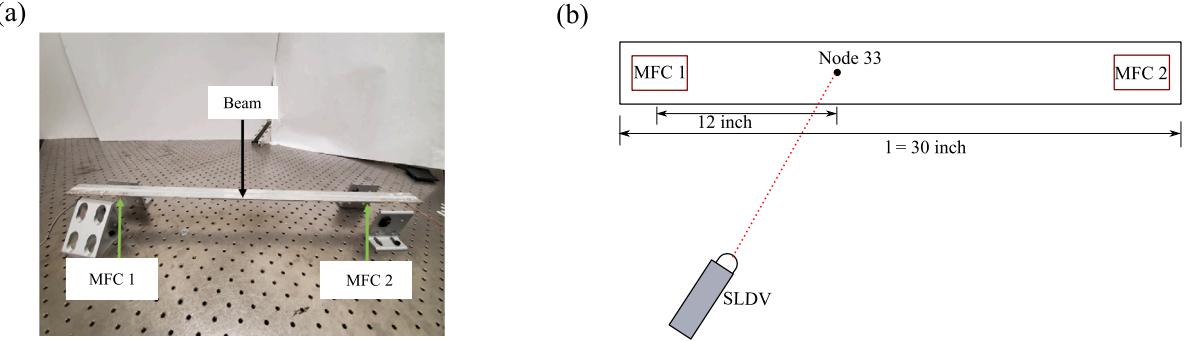


Fig. 11. Experimental setup used for the study (a) the picture of the free-free beam attached with MFC-1 and MFC-2, (b) schematic displaying the locations of MFC's on the beam and node 33.

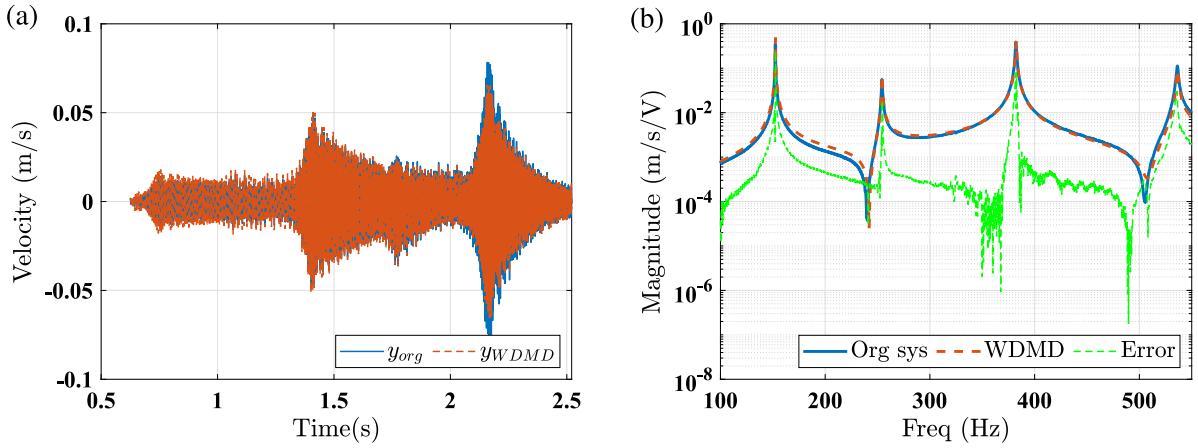


Fig. 12. Comparison of predicted WDMD response with the actual experimental data in (a) time domain and (b) frequency domain.

ten measured locations (nodal point 33) is compared with the SLDV measured velocity (solid blue line) in Fig. 12(a). Fig. 12(b) depicts the magnitude of the predicted FRF ( $\tilde{H}_{wdmd}(\omega)$ ) compared to the experimentally measured FRF ( $H(\omega)$ ) corresponding the same node. The high-fidelity fits in Figs. 12(a) and 12(b) demonstrate the efficacy of the algorithm in accurately reproducing the time domain and frequency domain characteristics of the beam under test. The relative error  $\epsilon_{td}^{rel} = 2.17 \times 10^{-1}$  is higher compared to the simulated data cases of the previous section, but this is expected because of the unfiltered experimental noise. Further studies are needed to further improve the robustness of WDMD methodology in cases with high experimental noise. It is important to note that employing ioDMD for the present experimental case study is not feasible since the internal states of the structure under test is unknown.

Similar to Section 4, we perform error convergence studies to evaluate the quality of the fit as a function of the number of output responses available to the algorithm. As before, the data-driven model's quality of the fit is evaluated using  $\epsilon_{td}^{rel}$  and  $\epsilon_{fd}^{rel}$  in time and frequency domain, respectively. The error convergence study is carried out by sequentially varying the number of outputs provided to the WDMD from 2 to 30. Fig. 13 shows the error convergence in both time and frequency domains. The relative error metrics  $\epsilon_{td}^{rel}$  and  $\epsilon_{fd}^{rel}$  converges at  $2.17 \times 10^{-1}$  and  $1.64 \times 10^{-1}$ , respectively, at  $d = 9$  and no further significant improvement in the quality of the fit is observed for  $d \geq 9$ . Nevertheless, the experimental studies clearly show the efficacy of WDMD methodology in accurately modeling the dynamic response of a beam.

## 5.2. Data-driven MIMO model

The algorithm is now experimentally tested for a MIMO case study using the same free-free beam excited by applying an input voltage to both MFC's simultaneously. The experimental setup and the procedure adopted follows a similar approach to the SIMO case with the only difference being multiple excitations.

Uncorrelated input chirp voltage signals provided to MFC 1 and MFC 2 excite the beam simultaneously. The chirp is designed to have different cycles of frequency sweeping to remove the mode cancellation arising due to correlated input signals. The WDMD methodology builds a MIMO, data-driven, state-space model using the collected response measurements. The learned model has

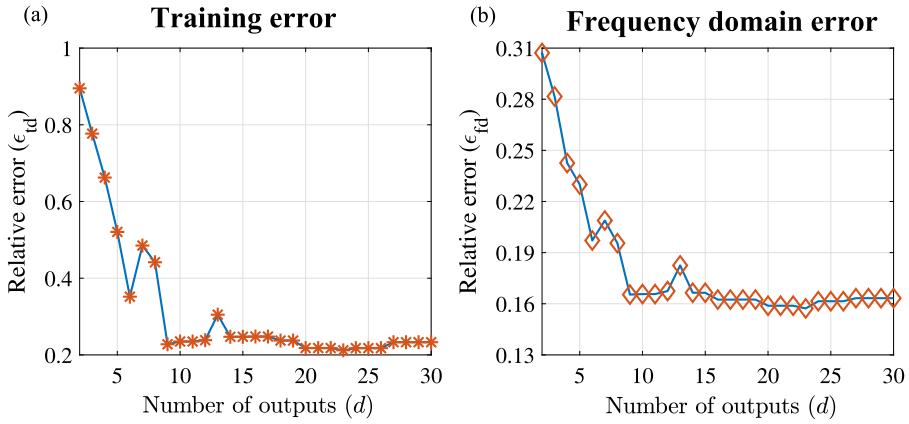


Fig. 13. Error convergence results for the experimental SIMO case study: (a) Relative time domain error for training phase and (b) Relative frequency domain error.

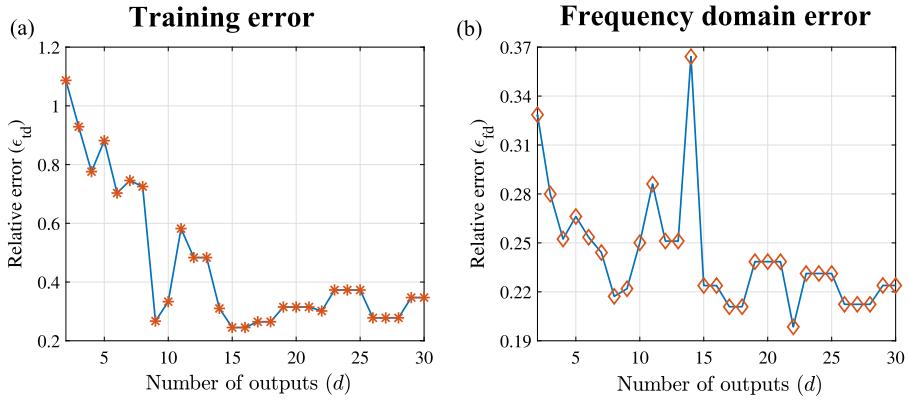


Fig. 14. Error convergence results for the experimental MIMO case study: (a) Relative time domain error for training phase and (b) Relative frequency domain error.

state-space dimensions  $\mathbf{A}_w \in \mathbb{R}^{140 \times 140}$ ,  $\mathbf{B}_w \in \mathbb{R}^{140 \times 2}$ ,  $\mathbf{C}_w \in \mathbb{R}^{10 \times 140}$  and  $\mathbf{D}_w \in \mathbb{R}^{10 \times 2}$ . The number of columns in matrix  $\mathbf{B}$  matrix represents the number of inputs in the system, which in the present MIMO example is two.

As in Section 5.1, the MIMO state-space model is excited with the training inputs to reproduce the results of the training phase. For brevity, the time domain and frequency domain fitting results for the model are not shown. Fig. 14 shows the time domain error  $\epsilon_{td}^{rel}$ , and the frequency domain  $\epsilon_{fd}^{rel}$  as a function of the number of outputs recorded and made available to the WDMD methodology. The lowest relative error value recorded is around 0.25, which is slightly higher than the SIMO case. Similar is the case for  $\epsilon_{fd}^{rel}$ , which has a lowest recorded value of 0.19, which is slightly higher than the SIMO case.

## 6. Conclusions and future work

The current study presented a novel data-driven methodology to model dynamical systems from its input–output trajectories, without having access to governing physical equations or full internal state dynamics. This was achieved using wavelets in conjunction with the ioDMD approach, leading to the proposed methodology, wavelet based DMD (WDMD). The numerical case study involving the dynamical response of a finite element cantilever beam was performed to demonstrate the effectiveness of WDMD. WDMD was utilized to develop a data-driven SIMO state-space dynamical model of the FEM beam based on measured input–output response. The WDMD methodology utilizes a subset of these measurements and approximates the underlying dynamics via a linear model using the maximal overlap discrete wavelet transform (MODWT) coefficients of the measured outputs as the auxiliary state-vector. The error convergence studies illustrated that even with a few measured outputs, WDMD was able to model the underlying dynamical system accurately. The experimental case study on a simple free-free beam, demonstrated the efficacy of WDMD methodology as an appropriate candidate for modeling practical dynamical systems despite having no access to internal state measurements.

The work presented herein demonstrates the feasibility of approximating the input–output dynamics of a vibrating beam based on measured input–output data using this new data-driven modeling approach. Although the WDMD algorithm performed reasonably

well in the presence of noise, additional analysis and numerical studies are required to better understand the performance of WDM in the case of noisy data and to improve its robustness. Furthermore, issues such as effect of sensor placement, input excitation requirements, sampling frequency, and the selection of wavelet decomposition level warrant further research.

### Declaration of competing interest

The authors declare that they have no known competing financial interests or personal relationships that could have appeared to influence the work reported in this paper.

### Data availability

Data will be made available on request.

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